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Optimal Control of a Linear Discrete System

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Optimal control of linear discrete dynamic systems with quadratic performance index is discussed. The optimal controller uses all states of the system. An additional constraint of using only the measurable output of the system is imposed. A suboptimal controller using only the measurable output of the system is derived. The tracking problem for a discrete system is also solved.

1. INTRODUCTION

Recently, increasing attention has been paid to the theory of systems; this is manifested by the great number of articles published all over the world. Application of this theory to the problems of control has led to the construction of new algorithms for the synthesis of dynamic systems which could not be obtained by classical methods in control engineering. Moreover, implementation of these algorithms necessitates utilization of digital computer.

In the well known literature [1], [2], [15], discussion is given of the synthesis of a continuous linear dynamic system (CLDS), i.e. determination of a feedback such that the control circuit fulfils our demands given by the specific performance criterion.

In recent literature [4], [5], [16], [13], a great deal of attention has been paid to the problems of synthesis of a CLDS using performance criterion formed by the integral of quadratic form of state and control of the system.

The present paper deals with the synthesis of a discrete linear dynamical system (DLDS). For determination of optimal discrete control we can use the dynamic programming approach [19] or the discrete maximum or minimum principle [20]. For determination of dynamic properties of a DLDS we shall use a state model which has state equation in the form

$$(1.1) \quad \mathbf{x}_{k+1} = \mathbf{M}\mathbf{x}_k + \mathbf{N}u_k,$$

$$(1.2) \quad \mathbf{y}_k = \mathbf{C}\mathbf{x}_k$$

where

$\mathbf{x}_k, \mathbf{u}_k, \mathbf{y}_k$ are n, r, m vectors of state, control, and output respectively at time k , $\mathbf{M}, \mathbf{N}, \mathbf{C}$ are $(n \times n), (n \times r)$ and $(m \times n)$ matrices of system, control, and output respectively the elements of which may be functions of time, and k is discrete time, $0, 1, 2 \dots$

For finite time K of control we assume that the performance criterion has the form

$$(1.3) \quad J_K = \frac{1}{2} \mathbf{x}_K^T \mathbf{S} \mathbf{x}_K + \frac{1}{2} \sum_{k=0}^{K-1} (\mathbf{x}_k^T \mathbf{Q} \mathbf{x}_k + \mathbf{u}_k^T \mathbf{R} \mathbf{u}_k)$$

where $\mathbf{Q}, \mathbf{S}, \mathbf{R}$ are symmetric positive semidefinite matrices of dimension $(n \times n), (n \times n), (r \times r)$ respectively (\mathbf{S} is a constant matrix). For infinite time of control, the performance criterion has the form

$$(1.4) \quad J = \frac{1}{2} \sum_{k=0}^{\infty} (\mathbf{x}_k^T \mathbf{Q} \mathbf{x}_k + \mathbf{u}_k^T \mathbf{R} \mathbf{u}_k)$$

where \mathbf{Q}, \mathbf{R} are constant symmetric positive semidefinite matrices.

In the second part of the present paper we shall derive relations for optimal feedback assuming that all states of the system are obtainable — we have so-called complete information about the state of the system. In the third part we discuss the tracking problem in the case of complete information.

In practical applications we cannot measure all states of the system and often it is not even economic to do so. In such case the designer can choose from various possibilities:

1. use reconstruction of state by observer - see [6], [7],
2. use reconstruction of state by Kalman-Bucy filter - see [2],
3. use only the output of system for control and thus control the system in a sub-optimal way.

The first and second cases utilizing reconstruction of the state of system have the disadvantage in increasing the order of the whole system.

The fourth part of this paper deals with the problem mentioned under item 3. A new algorithm is derived for solution of optimal feedback from the output of the system. In the fifth section, the tracking problem is solved in the case of incomplete information about the state of the system.

2. SYNTHESIS OF A DLDS WITH COMPLETE INFORMATION ABOUT THE STATE OF THE SYSTEM-CONTROL OF STATE

Given a DLDS described by state equations (1.1) and (1.2) and performance criterion (1.3). Using dynamic programming or the discrete minimum principle [8] we can

376 derive the optimal control law

$$(2.1) \quad \mathbf{u}_k^* = -\mathbf{G}_{K-k} \mathbf{x}_k^*$$

where

$$(2.2) \quad \mathbf{G}_{K-k} = (\mathbf{R} + \mathbf{N}^T \mathbf{K}_{K-k-1} \mathbf{N})^{-1} \mathbf{N}^T \mathbf{K}_{K-k-1} \mathbf{M}$$

is time dependent matrix of linear feedback and matrix \mathbf{K}_{K-k} satisfies the discrete form of Riccati equation

$$(2.3) \quad \mathbf{K}_{K-k} = \mathbf{Q} + \mathbf{M}^T \mathbf{K}_{K-k} \mathbf{M} - \mathbf{M}^T \mathbf{K}_{K-k-1} \mathbf{N} (\mathbf{R} + \mathbf{N}^T \mathbf{K}_{K-k-1} \mathbf{N})^{-1} \mathbf{N}^T \mathbf{K}_{K-k-1} \mathbf{M}.$$

Initial conditions for relations (2.2) and (2.3) are

$$(2.4) \quad \mathbf{G}_0 = \mathbf{0}, \quad \mathbf{K}_0 = \mathbf{S}.$$

Detailed derivation of these relations can be found for instance in [9].

In the case of infinite time of control with performance criterion in the form (1.4) and for a time invariant DLDS (1.1) and (1.2) relations (2.1) to (2.3) can be used in the limit for $K \rightarrow \infty$.

As shown in [8], matrices \mathbf{G}_{K-k} , \mathbf{K}_{K-k} may converge to finite values \mathbf{G} and \mathbf{K} . They really converge if the system is stabilizable. Then we have the following relation for optimal feedback

$$(2.5) \quad \mathbf{u}_k^* = -\mathbf{G} \mathbf{x}_k^*$$

where

$$(2.6) \quad \mathbf{G} = (\mathbf{R} + \mathbf{N}^T \mathbf{K} \mathbf{N})^{-1} \mathbf{N}^T \mathbf{K} \mathbf{M}$$

and \mathbf{K} is a symmetric positive definite matrix satisfying the discrete version of algebraic Riccati equation

$$(2.7) \quad \mathbf{K} = \mathbf{Q} + \mathbf{M}^T \mathbf{K} \mathbf{M} - \mathbf{M}^T \mathbf{K} \mathbf{N} (\mathbf{R} + \mathbf{N}^T \mathbf{K} \mathbf{N})^{-1} \mathbf{N}^T \mathbf{K} \mathbf{M}.$$

Equation (2.7) has only one positive semidefinite solution if the pair $(\mathbf{M}, \mathbf{Q}^{1/2})$ is observable.

These relations can be solved only using a digital computer especially in the case of systems of a higher order. Relations (2.2) and (2.3) can be programmed without difficulties if initial conditions (2.4) are known. If $\mathbf{S} = \mathbf{0}$, we can use the initial condition in the form

$$(2.8) \quad \begin{aligned} \mathbf{G}_1 &= \mathbf{0}, \\ \mathbf{K}_1 &= \mathbf{Q}. \end{aligned}$$

From the point of view of practical use it is more convenient to consider infinite

time of control. In that case we must solve the nonlinear matrix algebraic equations (2.6) and (2.7); there are two ways of solving them:

1. We can use relations (2.2) and (2.3) for the initial condition $\mathbf{K}_0 = 0$ and $\mathbf{G}_0 = 0$ and solve these relations for time $K \rightarrow \infty$. As a terminal condition we can use the relation

$$(2.9) \quad \|\mathbf{K}_{K-k} - \mathbf{K}_{K-k-1}\| \leq \varepsilon$$

where ε is a preset number of the order of 10^{-3} to 10^{-6} . Normally 30 to 40 iterations are sufficient to satisfy relation (2.9).

2. Relations (2.6) and (2.7) can be solved using the following algorithm mentioned in [10].

Theorem 1. Let \mathbf{V}_k , $k = 0, 1, 2, \dots$, be the solution of the equation

$$(2.10) \quad \mathbf{V}_k = \mathbf{M}_k^T \mathbf{V}_k \mathbf{M}_k + \mathbf{L}_k^T \mathbf{R} \mathbf{L}_k + \mathbf{Q}$$

where

$$(2.11) \quad \mathbf{L}_k = (\mathbf{R} + \mathbf{N}^T \mathbf{V}_{k-1} \mathbf{N})^{-1} \mathbf{N}^T \mathbf{V}_{k-1} \mathbf{M}, \quad k = 1, 2, \dots,$$

$$(2.12) \quad \mathbf{M}_k = \mathbf{M} - \mathbf{N} \mathbf{L}_k.$$

The matrix \mathbf{L}_0 must be chosen such that \mathbf{M}_0 be stable. This implies that the pair (\mathbf{M}, \mathbf{N}) must be stabilizable. Then

$$(2.13) \quad \mathbf{K} \leq \mathbf{V}_{k+1} \leq \mathbf{V}_k$$

and

$$(2.14) \quad \lim_{k \rightarrow \infty} \mathbf{V}_k = \mathbf{K}.$$

The proof of this algorithm is given in [10] where it is shown that the convergence rate is quadratic, i.e.

$$(2.15) \quad \|\mathbf{K} - \mathbf{V}_{k+1}\| \leq C \|\mathbf{K} - \mathbf{V}_k\|^2$$

where C is a constant which does not depend on the iteration index k .

This algorithm can be easily implemented on digital computer; for solving the linear matrix equation (2.10) the algorithm derived in [11] can be used. Solution of many examples on a digital computer has shown rapid convergence of this algorithm. Usually 4 or 5 iterations are sufficient for the difference $\|\mathbf{V}_k - \mathbf{V}_{k+1}\|$ to be less than 10^{-3} .

The only remaining problem is that of choosing the stabilization matrix \mathbf{L}_0 . Evidently for a stable system $\mathbf{L}_0 = 0$ can be chosen. Matrix \mathbf{L}_0 can also be chosen on the basis of physical interpretation of the problem. In general we can use algorithms for computation of the feedback matrix \mathbf{L}_0 such that eigenvalues of the matrix \mathbf{M}_0 be arbitrary. Practical algorithms and programmes are described in [12].

3. TRACKING PROBLEM FOR A DLDS WITH COMPLETE INFORMATION ABOUT THE STATE OF THE SYSTEM

In section 2 we assumed that the aim of control is the state vector $\mathbf{x} = 0$. In practical cases we often have to solve a problem with the target of control not in the origin of coordinates and it is demanded that the output \mathbf{y}_k of the system should track a given vector \mathbf{z}_k which may be either constant in time or time-dependent. For a CLDS this problem is discussed in [1], [12], [13]. For a DLDS we give here analogous algorithms, the derivation of which can be found in [9].

Let us define the error vector

$$(3.1) \quad \mathbf{e}_k = \mathbf{z}_k - \mathbf{y}_k.$$

We shall try to find a control vector \mathbf{u}_k giving the minimal value of performance index in the form

$$(3.2) \quad J_K = \frac{1}{2} \mathbf{e}_K^T \mathbf{S} \mathbf{e}_K + \frac{1}{2} \sum_{k=0}^{K-1} (\mathbf{e}_k^T \mathbf{Q} \mathbf{e}_k + \mathbf{u}_k^T \mathbf{R} \mathbf{u}_k)$$

where \mathbf{S} , \mathbf{Q} , \mathbf{R} are symmetric, positive semidefinite real matrices ($m \times m$), ($m \times m$) and ($r \times r$) respectively, \mathbf{S} is a constant matrix, and K is the time of control.

Using the discrete minimum principle or dynamic programming we can derive the optimal control law

$$(3.3) \quad \mathbf{u}_k^* = -(\mathbf{R} + \mathbf{N}^T \mathbf{K}_{k+1} \mathbf{N})^{-1} (\mathbf{N}^T \mathbf{K}_{k+1} \mathbf{M} \mathbf{x}_k^* + \mathbf{N}^T \mathbf{g}_{k+1})$$

where matrix \mathbf{K}_k satisfies the discrete version of Riccati equation

$$(3.4) \quad \mathbf{K}_k = \mathbf{C}^T \mathbf{Q} \mathbf{C} + \mathbf{M}^T \mathbf{K}_{k+1} \mathbf{M} - (\mathbf{N}^T \mathbf{K}_{k+1} \mathbf{M})^T (\mathbf{R} + \mathbf{N}^T \mathbf{K}_{k+1} \mathbf{N})^{-1} \mathbf{N}^T \mathbf{K}_{k+1} \mathbf{M}$$

and vector \mathbf{g}_k satisfies equation

$$(3.5) \quad \mathbf{g}_k = \mathbf{C}^T \mathbf{Q} \mathbf{z}_k + [\mathbf{M}^T - \mathbf{M}^T \mathbf{K}_{k+1} \mathbf{N} (\mathbf{R} + \mathbf{N}^T \mathbf{K}_{k+1} \mathbf{N})^{-1} \mathbf{N}^T] \mathbf{g}_{k+1}$$

with boundary conditions

$$(3.6a) \quad \mathbf{K}_K = \mathbf{C}^T \mathbf{S} \mathbf{C},$$

$$(3.6b) \quad \mathbf{g}_K = \mathbf{C}^T \mathbf{S} \mathbf{z}_K.$$

It is obvious from the form of the equations (3.4) to (3.6) that they can be solved starting from $k = K$ to $k = 0$. It means that this procedure can be used only if we know the values of the desired vector \mathbf{z}_k in the whole interval in advance. Moreover we are limited to finite time of control only.

In some cases, the tracking problem can be transformed into the problem of control of state. Let us suppose that the desired vector \mathbf{z}_k equals the solution of the

difference equation

$$(3.7) \quad \mathbf{z}_{k+1} = \mathbf{Fz}_k.$$

Let us define the extended vector \mathbf{w}_k of dimension $n + m$

$$(3.8) \quad \mathbf{w}_k = \begin{bmatrix} \mathbf{x}_k \\ \mathbf{z}_k \end{bmatrix}$$

which will be a state vector of the system described by state equations

$$(3.9) \quad \begin{aligned} \mathbf{w}_{k+1} &= \mathbf{Mw}_k + \mathbf{Nu}_k, \\ \mathbf{y}_k &= \mathbf{Cw}_k \end{aligned}$$

where matrices \mathbf{M} , \mathbf{N} , \mathbf{C} of dimensions $(n + m) \times (n + m)$, $(n + m) \times r$, $m \times (n + m)$ respectively have the form

$$(3.10) \quad \hat{\mathbf{M}} = \begin{bmatrix} \mathbf{M} & \mathbf{0} \\ \mathbf{0} & \mathbf{F} \end{bmatrix}, \quad \hat{\mathbf{N}} = \begin{bmatrix} \mathbf{N} \\ \mathbf{0} \end{bmatrix}, \quad \hat{\mathbf{C}} = [\mathbf{C} \ \mathbf{0}].$$

Tracking problem with performance criterion (3.2) can be transformed into a problem of control of state of the system (3.9) with the performance criterion

$$(3.11) \quad J_K = \frac{1}{2} \mathbf{w}_K^T \hat{\mathbf{S}} \mathbf{w}_K + \frac{1}{2} \sum_{k=0}^{K-1} (\mathbf{w}_k^T \hat{\mathbf{Q}} \mathbf{w}_k + \mathbf{u}_k^T \hat{\mathbf{R}} \mathbf{u}_k)$$

where matrices \mathbf{S} , \mathbf{Q} , \mathbf{R} are defined by

$$(3.12) \quad \hat{\mathbf{S}} = \begin{bmatrix} \mathbf{C}^T \mathbf{S} \mathbf{C} & -\mathbf{C}^T \mathbf{S} \\ -\mathbf{S} \mathbf{C} & \mathbf{S} \end{bmatrix}, \quad \hat{\mathbf{Q}} = \begin{bmatrix} \mathbf{C}^T \mathbf{Q} \mathbf{C} & -\mathbf{C}^T \mathbf{Q} \\ -\mathbf{Q} \mathbf{C} & \mathbf{Q} \end{bmatrix}, \quad \hat{\mathbf{R}} = \mathbf{R}.$$

If system (3.9) is not stabilizable, functional (3.11) does not converge for $K \rightarrow \infty$ and this procedure cannot be used for infinite time of control. When $\mathbf{F} = \mathbf{M}$ and $\text{rank}(\mathbf{C}) = m = n$, the tracking problem can always be transformed into a control-of-state problem even for infinite time of control.

4. SYNTHESIS OF A DLDS WITH INCOMPLETE INFORMATION ABOUT THE STATE OF THE SYSTEM

In sections 2 and 3 we assumed that all states of the system are measurable. It is often not possible in praxis and it is not even economic. In such a case one of the three possibilities mentioned in the introduction can be used.

In this and the following section we derive some new algorithms utilizing, for linear feedback, only the measurable output of the system.

Let us have a DLDS described by equations (1.1) and (1.2) and the performance criterion in the form

$$(4.1) \quad J_K = \frac{1}{2} \sum_{k=0}^{K-1} (\mathbf{x}_k^T \mathbf{Q} \mathbf{x}_k + \mathbf{u}_k^T \mathbf{R} \mathbf{u}_k)$$

where matrices \mathbf{Q} , \mathbf{R} are positive semidefinite.

Optimal control is assumed in the form

$$(4.2) \quad \mathbf{u}_k = -\mathbf{F}_k \mathbf{y}_k = -\mathbf{F}_k \mathbf{C} \mathbf{x}_k$$

where \mathbf{F}_k is the feedback matrix in the k -th step of control. Performance criterion (4.1) can then be written in the form

$$(4.3) \quad J_K = \frac{1}{2} \sum_{k=0}^{K-1} \mathbf{x}_k^T (\mathbf{Q} + \mathbf{C}^T \mathbf{F}_k \mathbf{R} \mathbf{F}_k \mathbf{C}) \mathbf{x}_k.$$

Solution of the state equation (1.1) with control (4.2) can be written in the form

$$(4.4) \quad \mathbf{x}_k = \Phi_k \mathbf{x}_0$$

where the state transition matrix has the form

$$(4.5) \quad \Phi_k = \prod_{i=0}^{k-1} (\mathbf{M} - \mathbf{N} \mathbf{F}_i \mathbf{C}), \quad k = 1, 2, \dots, K$$

and \mathbf{x}_0 is the initial state of the system.

From (4.5) it is obvious that matrix Φ_k satisfies the equation

$$(4.6) \quad \Phi_{k+1} = (\mathbf{M} - \mathbf{N} \mathbf{F}_k \mathbf{C}) \Phi_k, \quad \Phi_0 = \mathbf{I}.$$

Substituting relation (4.5) into (4.3) we obtain

$$J_K = \frac{1}{2} \sum_{k=0}^{K-1} \mathbf{x}_0^T \Phi_k^T (\mathbf{Q} + \mathbf{C}^T \mathbf{F}_k \mathbf{R} \mathbf{F}_k \mathbf{C}) \Phi_k \mathbf{x}_0$$

and utilizing relation $(\mathbf{x}^T \mathbf{A} \mathbf{x}) = \text{tr}(\mathbf{x} \mathbf{x}^T \mathbf{A})$

$$(4.7) \quad J_K = \frac{1}{2} \text{tr} \sum_{k=0}^{K-1} \mathbf{x}_0 \mathbf{x}_0^T \Phi_k (\mathbf{Q} + \mathbf{C}^T \mathbf{F}_k \mathbf{R} \mathbf{F}_k \mathbf{C}) \Phi_k.$$

Functional (4.7) depends on state transition matrix Φ_k , feedback matrix \mathbf{F}_k and also on initial state \mathbf{x}_0 .

Let us assume that the vector of initial state \mathbf{x}_0 is a random variable which satisfies the relations

$$(4.8) \quad E\{\mathbf{x}_0\} = 0, \quad E\{\mathbf{x}_0 \mathbf{x}_0^T\} = \mathbf{I}.$$

Criterion (4.7) is now a random variable. Evaluating the expected value of the performance criterion we obtain the modified performance measure in the form

$$(4.9) \quad \hat{J}_K = \frac{1}{2} E \sum_{k=0}^{K-1} \Phi_k^T (\mathbf{Q} + \mathbf{C}^T \mathbf{F}_k^T \mathbf{R} \mathbf{F}_k \mathbf{C}) \Phi_k.$$

In this way we have transformed the problem of minimizing criterion (4.1) from the space of states to the matrix space where matrix Φ_k corresponds to the state of the system, matrix \mathbf{F}_k corresponds to the control of the system and the system is described by equation (4.5). Instead of performance criterion (4.1) we shall minimize the expected value in (4.9).

This problem can be solved using dynamic programming [13]. Here we use the matrix minimum principle [17]. In the following derivation we use the identities [17]

$$(4.10) \quad \begin{aligned} \operatorname{tr} [\mathbf{ABC}] &= \operatorname{tr} [\mathbf{CAB}] = \operatorname{tr} [\mathbf{BCA}], \\ \frac{\partial}{\partial \mathbf{X}} \operatorname{tr} [\mathbf{AX}] &= \mathbf{A}^T, \\ \frac{\partial}{\partial \mathbf{X}} \operatorname{tr} [\mathbf{AX}^T] &= \mathbf{A}, \\ \frac{\partial}{\partial \mathbf{X}} \operatorname{tr} [\mathbf{X}] &= \mathbf{I}, \\ \frac{\partial}{\partial \mathbf{X}} \operatorname{tr} [\mathbf{X}^T] &= \mathbf{I}, \\ \frac{\partial}{\partial \mathbf{X}} \operatorname{tr} [\mathbf{AXBX}^T] &= \mathbf{AXB} + \mathbf{A}^T \mathbf{XB}^T. \end{aligned}$$

Let us define the Hamiltonian function by

$$(4.11) \quad H = \frac{1}{2} \operatorname{tr} [\Phi_k^T (\mathbf{Q} + \mathbf{C}^T \mathbf{F}_k^T \mathbf{R} \mathbf{F}_k \mathbf{C}) \Phi_k] + \operatorname{tr} [\mathbf{P}_{k+1}^T (\mathbf{M} - \mathbf{N} \mathbf{F}_k \mathbf{C}) \Phi_k].$$

The minimum of the Hamiltonian satisfies the condition

$$(4.12) \quad \frac{\partial H}{\partial \mathbf{F}_k} = 0.$$

From here it follows

$$(4.13) \quad \mathbf{0} = \mathbf{R} \mathbf{F}_k \mathbf{C} \Phi_k \Phi_k^T \mathbf{C}^T - \mathbf{N}^T \mathbf{P}_{k+1} \Phi_k^T \mathbf{C}^T.$$

Matrix \mathbf{P}_k is solution of the adjoint system

$$(4.14) \quad \mathbf{P}_k = \frac{\partial H}{\partial \Phi_k} = \mathbf{Q} \Phi_k + \mathbf{C}^T \mathbf{F}_k^T \mathbf{R} \mathbf{F}_k \mathbf{C} \Phi_k + (\mathbf{M} - \mathbf{N} \mathbf{F}_k \mathbf{C}) \mathbf{P}_{k+1}.$$

382 Let us assume that the constate matrix P_k has the form

$$(4.15) \quad P_k = K_k \Phi_k$$

and also

$$P_{k+1} = K_{k+1} \Phi_{k+1}.$$

Equaling the expressions (4.15) and (4.14) we get a difference equation for K_k

$$(4.16) \quad K_k = Q + C^T F_k^T R F_k C + (M - N F_k C)^T K_{k+1} (M - N F_k C).$$

Substituting (4.15) into (4.13) we can write

$$(4.17) \quad 0 = R F_k C \Phi_k \Phi_k^T C^T - N^T K_{k+1} (M - N F_k C) \Phi_k \Phi_k^T C.$$

Let us introduce a matrix L_k defined by the equation

$$(4.18) \quad L_k = \Phi_k \Phi_k^T.$$

From this (considering 4.6) the difference equation for L_k can be obtained as

$$(4.19) \quad L_k = (M - N F_{k-1} C) L_{k-1} (M - N F_{k-1} C)^T.$$

Substituting relation (4.18) into (4.17) the equation for optimal feedback matrix F_k is derived $F_k = (R + N^T K_{k+1} N)^{-1} N^T K_{k+1} M L_k C^T (C L_k C^T)^{-1}$. From here follows a theorem giving a necessary condition for optimality.

Theorem 2. Let F_k^* minimize the functional (4.9). Then

$$(4.20) \quad F_k^* = (R + N^T K_{k+1} N)^{-1} N^T K_{k+1} M L_k C^T (C L_k C^T)^{-1}$$

where

$$(4.21) \quad K_k = Q + C^T F_k^{*T} R F_k^* C + (M - N F_k^* C)^T K_{k+1} (M - N F_k^* C)$$

and

$$(4.22) \quad L_k = (M - N F_{k-1}^* C) L_{k-1} (M - N F_{k-1}^* C)^T.$$

Initial conditions for equations (4.21) and (4.22) are

$$(4.23) \quad L_0 = I, \quad K_{K-1} = Q, \quad F_{K-1} = 0.$$

Equations (4.21), (4.22) and (4.20) are nonlinear matrix difference equations whose solution is difficult. Convenient algorithm for digital computer has not been found yet.

Let us derive simple algorithms which would enable us to solve approximately

equations (4.20) and (4.21). Equation (4.17) for the feedback matrix F_k has the form 383

$$(4.24) \quad \mathbf{A} \cdot \mathbf{B} = \mathbf{0}$$

where

$$(4.25) \quad \begin{aligned} \mathbf{A} &= \mathbf{R}\mathbf{F}_k\mathbf{C} - \mathbf{N}^T\mathbf{K}_{k+1}\mathbf{M} + \mathbf{N}^T\mathbf{K}_{k+1}\mathbf{N}\mathbf{F}_k\mathbf{C}, \\ \mathbf{B} &= \Phi_k\Phi_k^T\mathbf{C}^T. \end{aligned}$$

Equation (4.24) has dimension $(r \times m)$ and has the solution for $(r \times m)$ elements of the feedback matrix F_k . Matrices \mathbf{A} and \mathbf{B} are divisors of zero but relation (4.24) is satisfied whenever $\mathbf{A} = \mathbf{0}$. This is a special solution of relation (4.24). According to [14] we can write a matrix equation

$$(4.26) \quad \mathbf{A} = \mathbf{A}$$

where \mathbf{A} is the error matrix. We want the error matrix to be minimal. Let us choose the criterion in the form

$$(4.27) \quad J_1 = \text{tr}(\mathbf{A}\mathbf{A}^T).$$

Now we derive the equation for feedback matrix F_k giving minimal value of criterion (4.27). Substituting (4.25) and (4.26) into relation (4.27) we obtain

$$(4.28) \quad \begin{aligned} J_1 = \text{tr} \{ &[(\mathbf{R} + \mathbf{N}^T\mathbf{K}_{k+1}\mathbf{N})\mathbf{F}_k\mathbf{C} - \mathbf{N}^T\mathbf{K}_{k+1}\mathbf{M}] \cdot \\ &\cdot [\mathbf{C}^T\mathbf{F}_k(\mathbf{R} + \mathbf{N}^T\mathbf{K}_{k+1}\mathbf{N}) - \mathbf{M}^T\mathbf{K}_{k+1}\mathbf{N}] \}. \end{aligned}$$

Denote

$$(4.29) \quad \begin{aligned} \mathbf{D} &= \mathbf{R} + \mathbf{N}^T\mathbf{K}_{k+1}\mathbf{N}, \\ \mathbf{E} &= \mathbf{N}^T\mathbf{K}_{k+1}\mathbf{M}. \end{aligned}$$

Equation (4.28) now has the form

$$J_1 = \text{tr}(\mathbf{D}\mathbf{F}_k\mathbf{C}\mathbf{C}^T\mathbf{F}_k^T\mathbf{D} - \mathbf{D}\mathbf{F}_k\mathbf{C}\mathbf{E}^T - \mathbf{E}\mathbf{C}^T\mathbf{F}_k^T\mathbf{D} + \mathbf{E}\mathbf{E}^T),$$

or

$$J_1 = \text{tr}(\mathbf{D}\mathbf{F}_k\mathbf{C}\mathbf{C}^T\mathbf{F}_k\mathbf{D}) - 2\text{tr}(\mathbf{D}\mathbf{F}_k\mathbf{C}\mathbf{E}^T) + \text{tr}(\mathbf{E}\mathbf{E}^T).$$

From the condition for J_1 to be minimal in every step of control it follows

$$(4.30) \quad \frac{\partial J_1}{\partial \mathbf{F}_k} = 0.$$

Using relations (4.10) we obtain $\mathbf{D}\mathbf{F}_k\mathbf{C}\mathbf{C}^T - \mathbf{E}\mathbf{C}^T = \mathbf{0}$.

From here it follows

$$(4.31) \quad \mathbf{F}_k = (\mathbf{R} + \mathbf{N}^T\mathbf{K}_{k+1}\mathbf{N})^{-1} \mathbf{N}^T\mathbf{K}_{k+1}\mathbf{M}\mathbf{C}^T(\mathbf{C}\mathbf{C}^T)^{-1}.$$

384 Utilizing criterion (4.27) in the form

$$(4.32) \quad J_1 = \text{tr}(\Delta \mathbf{V} \Delta^T)$$

where \mathbf{V} is a symmetric positive definite weighting matrix of dimension $(n \times n)$ we obtain the optimal value of the feedback matrix in the form

$$(4.33) \quad \mathbf{F}_k = (\mathbf{R} + \mathbf{N}^T \mathbf{K}_{k+1} \mathbf{N})^{-1} \mathbf{N}^T \mathbf{K}_{k+1} \mathbf{M} \mathbf{V} \mathbf{C}^T (\mathbf{C} \mathbf{V} \mathbf{C}^T)^{-1}.$$

Relations (4.31) to (4.33) for feedback matrix \mathbf{F}_k with relation (4.21) for matrix \mathbf{K}_k are easy to solve.

Theorem 2 gives only a necessary condition and so the uniqueness of the solution of equations (4.20)–(4.22) remains an open problem just as in the continuous version of this problem [18]. Results obtained using relations (4.31) or (4.33) do not guarantee the minimal value of criterion (4.10). Equation (4.31) is satisfied as nearly as possible in accordance with criterion (4.27) or (4.32).

5. TRACKING PROBLEM FOR A DLDS WITH INCOMPLETE INFORMATION ABOUT THE STATE OF THE SYSTEM

As in section 3 we shall now discuss the problem of tracking a given vector \mathbf{z}_k . Let us define the error vector

$$(5.1) \quad \mathbf{e}_k = \mathbf{z}_k - \mathbf{y}_k.$$

The control law has the form

$$(5.2) \quad \mathbf{u}_k = -\mathbf{F}_k \mathbf{y}_k = -\mathbf{F}_k \mathbf{C}_k \mathbf{x}_k.$$

The performance criterion for this problem has the form

$$(5.3) \quad J_K = \frac{1}{2} \mathbf{e}_K^T \mathbf{S} \mathbf{e}_K + \frac{1}{2} \sum_{k=0}^{K-1} (\mathbf{e}_k^T \mathbf{Q} \mathbf{e}_k + \mathbf{u}_k^T \mathbf{R} \mathbf{u}_k)$$

where matrices \mathbf{Q} , \mathbf{R} satisfy the same conditions as in section 3. After substitution and modification criterion (5.3) has the form

$$(5.4) \quad J_k = \frac{1}{2} (\mathbf{z}_k^T \mathbf{S} \mathbf{z}_k - 2 \mathbf{x}_0^T \Phi_k^T \mathbf{C}^T \mathbf{S} \mathbf{z}_k + \mathbf{x}_0^T \Phi_k^T \mathbf{C}^T \mathbf{S} \mathbf{C} \Phi_k \mathbf{x}_0) + \\ + \frac{1}{2} \sum_{k=0}^{K-1} (\mathbf{z}_k^T \mathbf{Q} \mathbf{z}_k - 2 \mathbf{x}_0^T \Phi_k^T \mathbf{C}^T \mathbf{Q} \mathbf{z}_k + \mathbf{x}_0^T \Phi_k^T \mathbf{C}^T \mathbf{Q} \mathbf{C} \Phi_k \mathbf{x}_0 + \mathbf{x}_0^T \Phi_k^T \mathbf{C}^T \mathbf{F}_k^T \mathbf{R} \mathbf{F}_k \mathbf{C} \Phi_k \mathbf{x}_0)$$

where matrix Φ_k satisfies relation (4.6),

$$(5.5) \quad \Phi_{k+1} = (\mathbf{M} - \mathbf{N} \mathbf{F}_k) \Phi_k, \quad \Phi_0 = \mathbf{I}.$$

We shall now evaluate the expected values for n linear independent initial vectors \mathbf{x}_0

satisfying the relation

$$(5.6) \quad \sum_{i=1}^n \mathbf{x}_{0i} \mathbf{x}_{0i}^T = I.$$

The modified performance criterion has now the form

$$(5.7) \quad \hat{J}_K = \frac{1}{2n} (n \mathbf{z}_K^T \mathbf{S} \mathbf{z}_K - 2 \sum_{i=1}^n \mathbf{x}_{0i}^T \Phi_K^T \mathbf{C}^T \mathbf{S} \mathbf{z}_K + \sum_{i=1}^n \mathbf{x}_{0i}^T \Phi_K^T \mathbf{C}^T \mathbf{S} \mathbf{C} \Phi_K \sum_{i=1}^n \mathbf{x}_{0i}) + \\ + \frac{1}{2n} \sum_{k=0}^{K-1} (n \mathbf{z}_k^T \mathbf{Q} \mathbf{z}_k - 2 \sum_{i=1}^n \mathbf{x}_{0i}^T \Phi_k^T \mathbf{C}^T \mathbf{Q} \mathbf{z}_k + \sum_{i=1}^n \mathbf{x}_{0i}^T \Phi_k^T \mathbf{C}^T \mathbf{Q} \mathbf{C} \Phi_k \sum_{i=1}^n \mathbf{x}_{0i} + \\ + \sum_{i=1}^n \mathbf{x}_{0i}^T \Phi_k^T \mathbf{C}^T \mathbf{F}_k^T \mathbf{R} \mathbf{F}_k \mathbf{C} \Phi_k \sum_{i=1}^n \mathbf{x}_{0i}).$$

Let us assume that

$$(5.8) \quad \sum_{i=1}^n \mathbf{x}_{0i}^T = [1, 1, \dots, 1].$$

As in [13] let us define a symmetric matrix of dimension $(m \times m)$

$$(5.9) \quad \bar{\mathbf{Z}}_k = n \mathbf{z}_k \mathbf{z}_k^T$$

and a matrix $(m \times n)$

$$(5.10) \quad \tilde{\mathbf{Z}}_k = \mathbf{z}_k \sum_{i=1}^n \mathbf{x}_{0i}^T.$$

After substitution of (5.8), (5.9), (5.10) into (5.7) the performance criterion now has the form

$$(5.11) \quad J_K = \frac{1}{2n} \text{tr} [\Phi_K^T \mathbf{C}^T \mathbf{S} \mathbf{C} \Phi_K + \bar{\mathbf{Z}}_K \mathbf{S} - 2 \tilde{\mathbf{Z}}_K \Phi_K \mathbf{C}^T \mathbf{S}] + \\ + \frac{1}{2n} \text{tr} \left[\sum_{k=0}^{K-1} (\Phi_k^T (\mathbf{C}^T \mathbf{Q} \mathbf{C} + \mathbf{C}^T \mathbf{F}_k \mathbf{R} \mathbf{F}_k \mathbf{C}) \Phi_k + \bar{\mathbf{Z}}_k \mathbf{Q} - 2 \tilde{\mathbf{Z}}_k \Phi_k^T \mathbf{C}^T \mathbf{Q}) \right].$$

This modified performance criterion (5.11) must be minimized by \mathbf{F}_k subject to the constraint imposed by the system equation (5.5).

For the solution we shall again use the discrete matrix minimum principle. The constant $1/n$ in (5.11) has been left out for reasons of simplicity. The Hamiltonian for this problem is

$$(5.12) \quad H = \frac{1}{2} \text{tr} [\Phi_k^T (\mathbf{C}^T \mathbf{Q} \mathbf{C} + \mathbf{C}^T \mathbf{F}_k \mathbf{R} \mathbf{F}_k \mathbf{C}) \Phi_k + \bar{\mathbf{Z}}_k \mathbf{Q} - 2 \tilde{\mathbf{Z}}_k \Phi_k^T \mathbf{C}^T \mathbf{Q}] + \\ + \text{tr} [(M - N \mathbf{F}_k \mathbf{C}) \Phi_k \mathbf{P}_{k+1}^T].$$

Necessary condition of optimality is

$$(5.13) \quad \frac{\partial H}{\partial \mathbf{F}_k} = \mathbf{R} \mathbf{F}_k \mathbf{C} \Phi_k \Phi_k^T \mathbf{C}^T - N^T \mathbf{P}_{k+1} \Phi_k^T \mathbf{C}^T = \mathbf{0}.$$

386 Matrix P_k is the solution of the adjoint systems

$$(5.14) \quad P_k = \frac{\partial H}{\partial \Phi_k} = (C^T Q C + C^T F_k^T R F_k C) \Phi_k - 2C^T Q \tilde{Z}_k + (M - N F_k C)^T P_{k+1}.$$

From the transversality conditions it follows that

$$(5.15) \quad P_K = C^T S C \Phi_K - C^T S \tilde{Z}_K.$$

Let us assume that the matrix P_k can be written in the form

$$(5.16) \quad P_k = K_k \Phi_k - G_k$$

where the unknown matrix G_k is connected with the reference input z_k . Equating equations (5.16) and (5.14) we get difference equations for matrices K_k and G_k .

$$(5.17) \quad \begin{aligned} K_k &= C^T Q C + C^T F_k^T R F_k C + (M - N F_k C)^T K_{k+1} (M - N F_k C), \\ G_k &= 2C^T Q \tilde{Z}_k + (M - N F_k C)^T G_{k+1}. \end{aligned}$$

From (5.15) we obtain the boundary conditions

$$(5.18) \quad K_K = C^T S C, \quad G_K = C^T S \tilde{Z}_K.$$

The optimal output feedback F_k follows from equation (5.13)

$$(5.19) \quad R F_k C \Phi_k \Phi_k^T C^T - N^T [K_{k+1} (M - N F_k C) \Phi_k - G_{k+1}] \Phi_k^T C^T = 0.$$

From here it follows

$$(5.20) \quad F_k = (R + N^T K_{k+1} N)^{-1} N^T (K_{k+1} M \Phi_k - G_{k+1}) \Phi_k^T C^T (C \Phi_k \Phi_k^T C^T).$$

The optimal feedback gain can thus be divided into two parts. One is identical with the feedback gain designed for the state regulator problem-equation (4.20), the second part is determined by reference input z_k only.

In case where the initial value z_0 of the vector z_k can be considered to be a random variable as well it can be shown that the tracking problem can be transformed into the state regulator problem. Let us assume that vector z_k is a solution of the difference equation

$$(5.21) \quad z_{k+1} = H z_k.$$

Let us define the extended state vector

$$(5.22) \quad w_k = \begin{bmatrix} x_k \\ z_k \end{bmatrix}.$$

Equation for the original system (1.1) and the equation (5.21) can be put together and using (5.22) we obtain

$$(5.23) \quad w_{k+1} = \begin{bmatrix} M & 0 \\ 0 & H \end{bmatrix} w_k + \begin{bmatrix} B \\ 0 \end{bmatrix} u_k.$$

Let the output of the system (5.23) be

$$(5.24) \quad \bar{y}_k = \bar{C} w_k,$$

where

$$\bar{C} = [C, -I].$$

It follows that

$$(5.25) \quad \bar{y}_k = y_k - z_k = -e_k.$$

The tracking problem for the original system is equivalent to the output regulator problem for the system (5.23) and (5.24).

6. CONCLUSION

In the present paper the problem of optimal control of a DLDS with respect to quadratic performance criterion is solved.

When all state of the system are measurable, solution of this problem is well known and is discussed in section 2. Algorithms convenient for digital computer are also mentioned here.

When the additional constraint of using only the measurable output is imposed we have the so called problem of incomplete information about the state of the system. Optimal solution of this problem uses state reconstruction by an additional dynamic system (observer or Kalman-Bucy filter) whose dimension is specified.

In optimal solution we can use dynamic controller of a lower dimension that is necessary for state reconstruction. In this paper the limiting problem is solved where the regulator is only proportional and uses only the measurable output of the system. This suboptimal controller is derived assuming the initial state of the system has some statistical properties. Solution of this problem results in nonlinear matrix equations solving of which is difficult. A simplified but approximate solution of this problem is discussed at the end of section 4. Like in the continuous version [18] questions about the existence and the uniqueness of the solution of the suboptimal proportional feedback controller are yet to be answered.

The discrete version of the tracking problem both for complete and incomplete information about the state of the system is also solved in the present paper.

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- [1] Athans M., Falb L. P.: Optimal control. McGraw Hill, N. York 1966.
- [2] Kalman R. E., Falb P. L., Arbib M. A.: Topics in mathematical system theory. McGraw Hill, N. York 1969.
- [3] Desoer Ch. A., Zadeh L. A.: Linear system theory. McGraw Hill, N. York 1963.
- [4] Athans M., Levine W.: On the design of linear system using only output variable feedback. In: Proc. 6th Allerton Conf. Circuit and system theory 1969, 661–670.
- [5] Athans M., Johnson T.: On the determination of the optimal constrained dynamic compensator for linear constant system. IEEE Tran. on Automatic Control *AC-15* (1970), 6, 658–660.
- [6] Mitter S. K., Foulkes R.: Controllability and pole assignment for discrete time linear systems defined over arbitrary fields. SIAM Journal of control *9* (1971), 1, 1–8.
- [7] Tse Edison: Optimal minimal order observer estimators for discrete linear time varying systems. IEEE Tran. on Automatic Control *AC-15* (1970), 4, 416–426.
- [8] Dorato P., Levis A. H.: Optimal linear regulator: The discrete time case. IEEE Tran. on Automatic Control *AC-16* (1971), 6, 613–620.
- [9] Kozáčíková A.: Algorithms for solution of linear discrete systems with incomplete information about the state of the system. Thesis, ČVUT, Praha 1972.
- [10] Hewer G. A.: An iterative technique for the computation of the steady-state gains for the discrete optimal regulator. IEEE Tran. on Automatic Control *AC-16* (1971), 4, 382–383.
- [11] Štecha J., Kozáčíková A., Kozáčík J.: Solution of matrix equations $PA + A^T P = -Q$ and $M^T P M - P = -Q$ resulting in Lyapunov stability analysis. Kybernetika *9* (1973), 1, 62–71.
- [12] Kozáčík J.: Algorithms for solution of linear continuous systems with incomplete information about the state of the system. Thesis, ČVUT, Praha 1972.
- [13] Fink M., Štecha J.: Synthesis of linear dynamic systems with incomplete information about the state. Kybernetika *7* (1971), 6, 467–491.
- [14] Bjerhmmar A.: A generalized matrix algebra. Bulletin No. 9 from the Division of geodesy, Stockholm 1958.
- [15] Понтрягин В. С.: Математическая теория оптимальных процессов. Физматгиз, Москва 1961.
- [16] Athans M., Levine W. S.: On the determination of the optimal constant output feedback gains for linear multivariable systems. IEEE Tran. on Automatic Control *AC-15* (1970), 1, 44–48.
- [17] Athans M.: The matrix minimum principle. Information and Control *11* (1967), 6, 592–606.
- [18] Athans M., Levine W. S., Johnson T.: Optimal limited state variable feedback controllers for linear systems. IEEE Tran. on Automatic Control *AC-16* (1971), 6, 785–793.
- [19] Bellman R.: Dynamic programming. Princeton University Press, Princeton 1957.
- [20] Liang-Tseng Fan, Chin-Sen Wang: The discrete maximum principle. John Wiley, N. York 1964.
- [21] Lidický J.: Optimal discrete control of linear continuous systems. Thesis, ČVUT, Praha 1971.

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